A Versatile Power Converter for High-Frequency Link Systems

PRADEEP K. SOOD, MEMBER, IEEE, THOMAS A. LIPO, FELLOW, IEEE, AND IRVING G. HANSEN

Abstract—A single-phase high-frequency link appears to be an attractive alternative to the dc link commonly employed in power conversion systems. This paper proposes a power converter suitable for one-step conversion of the single-phase high-frequency link voltage to the three-phase low-frequency voltages typically required for interfacing with system sources and loads. The converter utilizes zero voltage switching principles to minimize switching losses and uses an easy to implement technique of pulse density modulation for the control of the amplitude, frequency, and waveshape of the synthesized low-frequency signals. Adaptation of the proposed topology for power conversion to single-phase ac and dc voltage or current outputs is shown to be straightforward. The feasibility of the proposed power circuit and the control technique have been experimentally verified.

I. INTRODUCTION

POWER conversion systems typically utilize dc voltage or current links for power distribution to the input and output converters and to support temporary energy storage requirements of the converters. Recently, however, use of a single-phase high-frequency (20 kHz or more) sinusoidal voltage bus as a link has been proposed as an alternative to the dc link approach [1], [2], [3]. A high-frequency ac link allows the flexibility of adjusting the link voltage according to the individual needs of the load/source together with easy electrical isolation for safer grounding or noise suppression by means of compact and lightweight transformers on the link side of the converters. In addition, high-frequency link systems show potential improvements in such performance areas as speed of response of the component converters, overall system levels of audible noise, interference at lower frequencies, safety and reliability, and compatibility with high-frequency machines.

Interface Converter Requirements

As in any link system, power converters are invariably needed to interface system loads and source to the link since few loads sources are able to operate directly from the link as a power source. Performance of the overall power conversion system depends to a large extent on the capability of these power converters to effectively and efficiently perform this interface function. In general, the following characteristics can be considered desirable in power converters used as interface converters in the high-frequency link systems:

- high efficiency for increased system efficiency and for reduced size and weight of the heat dissipating components;
- inherent bidirectional power flow capability (not requiring substantial modifications in the power circuit for reverse power flow);
- low distortion output waveform with fundamental frequencies as high as 1000 Hz for increased power density of associated mechanical systems;
- simple and reliable means of controlling converter output voltage and frequency;
- minimum voltage or frequency disturbances to the link;
- adaptability to different types of loads/sources for a higher level of uniformity and reliability in the system.

Limitation of Familiar Converter Topologies

Converters not designed specifically for operation from a high-frequency link are unlikely to perform adequately as interface converters for high-frequency link systems. Consider, for exmaple, the phase-controlled converter (cycloconverter) which is frequently used when one-step power conversion from an ac voltage source is required. A major limitation of such a converter in a high-frequency link system would be the excessive switching losses resulting from a high switching rate (forty thousand switches per second for a 20-kHz link) and an inherently high loss per switching of the phase-angle control scheme. In addition, phase-controlled converters cause a varying (and lagging, if naturally commutated) current to be returned to the link, making it more difficult to regulate the link, and contain objectionable levels of dv/dt's in the generated voltage waveforms.

Intermediate dc link converters are possible which might operate by converting the high-frequency link power to an intermediate dc form from which another dc input converter would then generate the desired low-frequency ac or adjustable amplitude dc. However, such two-

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P. K. Sood was with the University of Wisconsin, Madison, WI. He is now with Emerson Electric Co., 12301 Missouri Bottom Road, P.O. Box 3946, St. Louis, MO 63136.

T. A. Lipo is with the University of Wisconsin, Department of Electrical and Computer Engineering, 1415 Johnson Dr., Madison, WI 53706.

I. G. Hansen is with the NASA Lewis Research Center, 2100 Brookpark Rd., Cleveland, OH 44135.

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stage topologies are inherently less efficient and tend to have limited capabilities in such aspects of converter performance as output frequency limit, converter bandwidth, ease of protection, reliability, and others, due to the "hard" switching used in dc link converters. Resonant techniques are being increasingly employed to eliminate or reduce these drawbacks [4], [5], [6]. However, there appears to be some difficulty in using resonant converter topologies for bidirectional power transfer from an existing high-frequency voltage.

This paper describes a power conversion technique which takes advantage of, instead of being limited by, the high frequency of the link. Utilizing this conversion technique, a class of one-step bidirectional power converters are proposed that are suitable for interfacing a wide variety of sources and loads to the high-frequency link.

II. PROPOSED POWER CONVERSION TECHNIQUE

It is clear that the link voltage in an ac link system crosses through zero twice per cycle of the link frequency. By restricting all switching in the converter operating directly from the link to these zero crossing points, converter switching losses can be made small and switching related device voltage stresses are minimized. Purely capacitive (hence lossless) snubbers can be used when needed, and the generated voltage waveforms become free of abrupt transients seen in phase-controlled converters. In addition, zero voltage switching causes the current returned to the link to be always in phase (or 180 degrees out of phase) with the link voltage, which makes control of the frequency and distortion of the link voltage easier. Recently reported work [7], [8] shows that the advantages of zero voltage switching are being more widely recognized and will find applications outside of ac link systems discussed here.

Zero voltage switching in a fixed-frequency system creates a fixed converter switching rate. This requires that new modulation strategies be developed to allow control of frequency, amplitude, and waveshape of the low-frequency signal synthesized from the high-frequency voltage of the link. The technique of area comparison—pulse density modulation has been suggested earlier by the authors [3] for this purpose and will be reviewed here briefly.

III. REVIEW OF PULSE DENSITY MODULATION (PDM)

Fig. 1 illustrates the principle of the zero voltage switching constraint and how a one-stage power converter is used to generate a low-frequency voltage component by synthesizing the desired fundamental component from complete half cycles of the high-frequency link voltage. It is clear that such low-frequency waveforms can be synthesized either by programmed logic (analogous to programmed pulsewidth modulation (PWM) for dc link systems) or, it can be generated using a type of modulation scheme (analogous to the sine-triangle PWM).

Fig. 2 shows the block schematic of one such modulation scheme based on the concept of *area comparison*. In this scheme, the area under the reference signal is compared with the area of the synthesized signal. If the comparison indicates that the area of the synthesized signal is more (less) than desired, then the controller causes the next half-cycle pulse to be omitted (applied) so that this area is decreased (increased). In this manner, voltages or currents having a fundamental component of dc, sinusoidal ac, or any other smooth waveform may be synthesized using a single integrator, a comparator, and a few logic gates. This simple implementation results in the density of the half-cycle pulses in the synthesized voltage to be modulated in close accordance with the amplitude of the reference signal. The term *area comparision—pulse density modulation* (AC-PDM) has been used to differentiate this scheme from other PDM schemes and possible programmed methods of generating such waveforms.

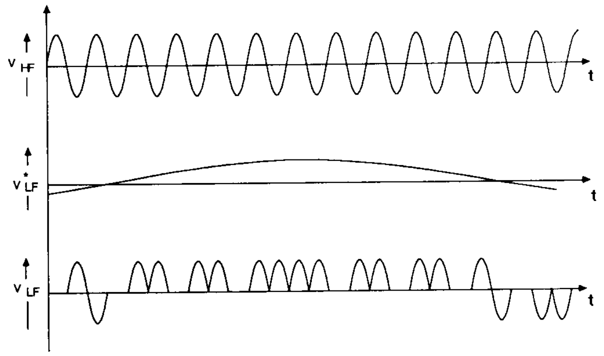


Fig. 1. Pulse-density-modulated (PDM) synthesis of low-frequency voltage.

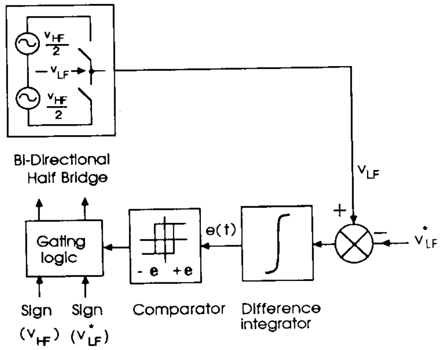


Fig. 2. Area comparison—pulse density modulation (AC-PDM) scheme.

It has previously been shown [3] that if the link frequency is sufficiently high (by a factor of 20 or more) and if the modulation index does not exceed unity, then the synthesized signals have very little low-order distortion for a wide range of frequency and amplitude of the synthesized signal. Also, the high-frequency harmonics occur only as the side band of the switching frequency where they pose no problem to most loads/sources. The spectral characteristics over the intermediate frequency range tend to be nearly flat. This broad band spectrum over the audio range produces lower and easier to tolerate audible noise levels in ac machines operated from PDM converters.

IV. THREE-PHASE AC BRIDGE INTERFACE CONVERTER

Based on the zero voltage switching PDM power conversion technique, topologies for conversion of single-phase high-frequency voltage to three- or single-phase dc or ac low-frequency voltage or currents can be visualized. The three-phase case has been considered initially because it represents the general case of down conversion from a high-frequency link. Synthesis of single-phase ac can be visualized as restricting the number of phases on the low-frequency side of the three-power converter. An additional restriction of zero frequency then degenerates into the case of dc voltage or current synthesis.

Although other three-phase power circuit topologies are possible [9], discussion here will be limited to a three-phase ac bridge circuit which can be derived from the dc link three-phase bridge circuit by direct analogy.

Topologic Equivalence to the DC Link Bridge

Fig. 3 shows the dc link bridge converter which is well-known as the minimal power structure for transforming dc power to three-phase voltages or currents of controllable frequency and amplitude. A shunt filter (large electrolytic capacitor) provides a low-impedance path to the harmonics in the current returned to the link by the switching action of the power circuit. As a result, the distortion (resulting ripple) of the link voltage is kept to a minimum. Once charged, the shunt filter offers a high impedance to the current of the link frequency (dc current).

Fig. 4 shows the three-phase ac bridge. Like the dc bridge, it is a minimal topology consisting of six hybrid switches (now with reverse voltage blocking capability). The ac bridge also operates from fixed frequency and the regulated voltage of the link to generate three-phase voltages or currents of controllable frequency and amplitude. The bridge must again have a filter on the link side for circulating harmonic currents. One possible filter configuration for this purpose is a shunt connected *LC* tank circuit resonant at the frequency of the link. Once "charged," the tank circuit offers a high impedance to the current of the link frequency and a lower impedance to currents of all frequencies. The size of this tank circuit determines the amount of fluctuations ("ripple") in the link voltage in much the same manner as for the dc link system.

Voltage Conversion Ratio

The output to input voltage ratio of the three-phase PDM bridge converter can be derived as follows. Reference [3] gives the expression for the fundamental voltage that can be realized by a half-bridge circuit before the AC–PDM controller begins to saturate as

$$V_{\mathrm{LF\,max}} = \frac{V_{\mathrm{HF}}}{\pi} \tag{1}$$

where $V_{\mathrm{LF\,max}}$ is the maximum level of the dc signal or the peak value of an ac signal which can be synthesized from a high-frequency link voltage of peak value V_{HF}. The maximum rms fundamental line voltage is thus given as

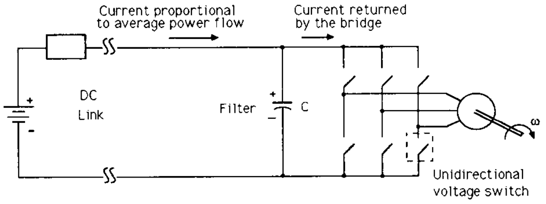


Fig. 3. DC link bridge converter.

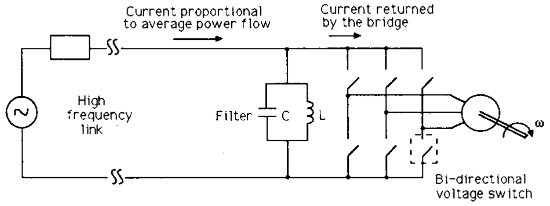


Fig. 4. Bridge converter with ac link.

$$v_{l-l\,\mathrm{max}} = \frac{\sqrt{3}\,v_{\mathrm{HF}}}{\pi} \tag{2}$$

where v_{HF} is the rms value of the link voltage. Finally, the ratio of these two rms quantities is

$$\frac{v_{l-l\,\mathrm{max}}}{v_{\mathrm{HF}}} = \frac{\sqrt{3}}{\pi}. \tag{3}$$

Equation 3 shows that no more than 55 percent of the link rms voltage can be converted to line voltage on the low-frequency side before the PDM controller begins to saturate. Conversely, for one per-unit line voltage at the converter output, the link voltage must be 1.8 times larger. To provide some basis for comparison, similar ratios have been computed for PWM dc link converters and for a recently proposed "resonant dc link" converter [7] which seeks to eliminate the losses and stresses associated with the "hard" switching of the dc link converters by using resonant zero voltage switching but retains its unipolar link structure. Table I shows the voltage conversion ratios along with the theoretical voltage ratings required of devices for each type of converter. Note that practical constraints such as dead times, device safety factors to account for snubber overshoots, etc. can significantly affect the comparison. In general, zero voltage switching converters are much less prone to derating because of these factors due to the reduced voltage near switching instants and the lack of snubber overshoots. Clearly, a reduced value of the voltage conversion ratio is the trade-off for dramatic improvements in switching performance seen in zero voltage switching converters. Note that the ac link PDM converter offers an excellent compromise in this regard.

Converter Power Switches

It may appear that an ac bridge operating from a high-frequency link would require a large number of very spe-

TABLE I
COMPARISON OF VOLTAGE CONVERSION RATIOS AND DEVICE VOLTAGE RATINGS FOR THREE HIGH-PERFORMANCE CONVERTERS

Inverter Type	Max. Fundamental Pole Voltage (peak)	Max. Fundamental Line Voltage (rms)	Line Voltage to Link Voltage Ratio (rms/rms)	Device Voltage to Line Voltage Ratio (peak/rms)
DC link PWM	$\frac{1}{2}V_d$	$\frac{\sqrt{3}}{2\sqrt{2}}V_d$	$\frac{\sqrt{3}}{2\sqrt{2}} = 0.612$	$\frac{2\sqrt{2}}{\sqrt{3}} = 1.6$
AC link PDM	$\frac{1}{\pi}V_p$	$\frac{\sqrt{3}}{\pi\sqrt{2}}V_p$	$\frac{\sqrt{3}}{\pi} = 0.551$	$\frac{\pi\sqrt{2}}{\sqrt{3}} = 2.56$
Resonant dc link PDM	$\frac{1}{4}V_p$	$\frac{\sqrt{3}}{4\sqrt{2}}V_p$	$\frac{1}{2}$	$\frac{4\sqrt{2}}{\sqrt{3}} = 3.27$

cial devices making the power circuit complex and unreliable. This need not be the case. The device capabilities needed for a PDM bridge operating from a link frequency in the neighborhood of 20 kHz are not markedly different from those needed in the present day PWM inverters operating at switching frequencies nearly one order of magnitude lower. This is because the switching frequency in PWM converters is limited primarily by high losses and high device stresses generated as a result of "hard" switching from the dc link. The zero voltage switching used in the PDM converters drastically reduces these stresses. The number of devices needed should also not pose any serious difficulty because the same considerations (minimization of stray leakage, ease of manufacturing, reliability etc.) that led to the evolution of the present day hybrid switches for PWM converters (transistor-reverse diode or GTO-reverse diode, etc.) can be expected to eventually produce similar hybrid realizations suitable for converters operating from an ac link.

Operation with Natural Commutation

Automatic reversal of the ac link voltage offers an opportunity to also naturally commutate the devices in a PDM converter. However, the need to establish circulating current of appropriate polarity to achieve turn-off of the conducting device now causes the converter operation to become somewhat dependent on the power factor at the low-frequency end. In particular, when the power flow in the converter is in the direction of the high-frequency link, incoming switches have to be activated in advance of the voltage reversal to ensure circulating current of the correct polarity to turn off the outgoing devices. This advance firing increases the distortion of the link voltage and the voltage synthesized on the low-frequency end. It also increases the switching losses in the converter. However, if the load power factor is high then the advance firing is limited to relatively few of the high-frequency high-cycles of the generated signal. Naturally commutated PDM converters may be used without a major deterioration of converter characteristics.

Link Filter

The parallel connected *LC* tank circuit tuned to the link frequency functions in an ac link system much like the electrolytic capacitor of a dc link system. By locating the capacitor of the tank circuit close to the PDM converter power bus, a low-impedance path is provided which shunts the high-frequency components of the current returned by the converter to the link. The tank filter also stores energy which helps meet the pulsating instantaneous power need of the PDM converter. The effectiveness of this power averaging by such a filter depends on such factors as the filter configuration and capacity, the frequency characteristics of the link impedance, the converter circuit topology, and the number of converters operating simultaneously from the link. The size of the required filter can vary depending upon these factors and the amount of voltage "ripple" that can be tolerated. In this respect, each system must be optimized to meet its individual requirement. Alternate filter topologies and optimization procedures for a given system's requirements appear to be areas for further study.

AC-PDM Tolerance to Link Voltage Ripple

The desire to minimize the size and losses associated with the PDM filter suggests that there will always be some "ripple" variations in the link voltage. Fortunately, the AC-PDM is a closed-loop control scheme and automatically compensates for link voltage variations whether they be on a cycle by cycle basis or they be the slow variations in the "average" amplitude.

V. CONVERTER OPERATION

A PDM converter can generate a balanced set of three-phase voltages with sinusoidal fundamental component whose amplitude and frequency can be controlled independently. Such a synthesized set of voltages can supply a passive *FL* load or be used to interface an ac machine to the high-frequency link. We shall limit the discussion here to operation of an induction machine with power flow in either direction.

Interfacing Induction Machines

Using computer models (see [9] for discussion of these models) of an induction machine, PDM converter interface has been studied. A 400-Hz 210-V three-phase machine having parameters (Table II) typical of a machine in its class has been assumed. The converter output fre-

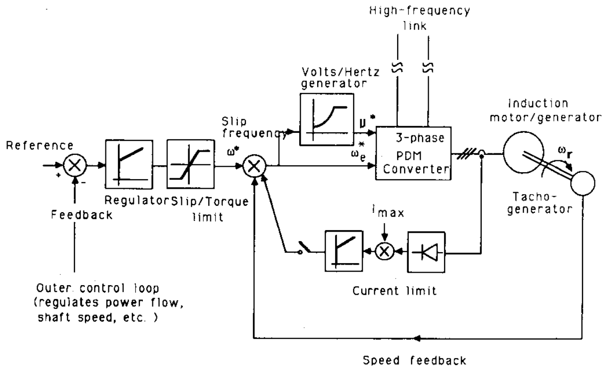


Fig. 5. Block diagram of slip controller.

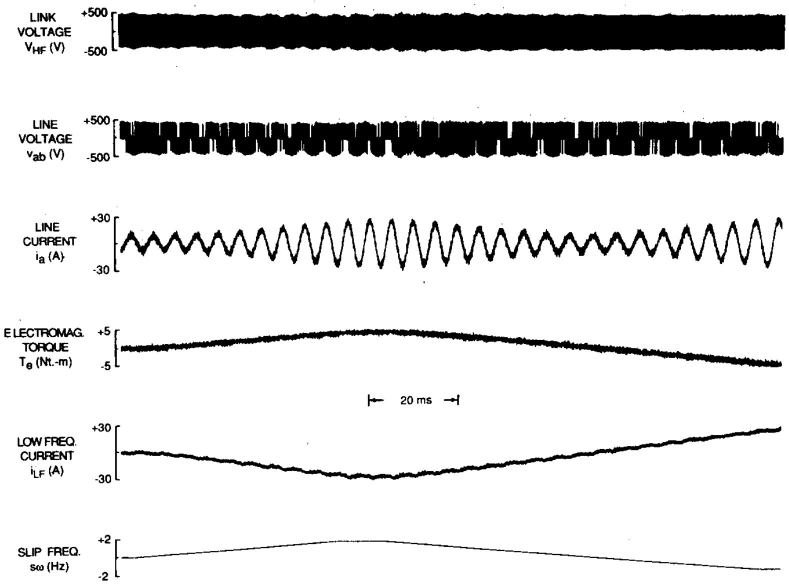


Fig. 6. Motor/generator operation of induction machine supplied from high-frequency link PDM converter.

TABLE II

INDUCTION MACHINE PARAMETERS USED IN SIMULATION STUDY

Rated power	7.5 HP
Rated voltage	210 V
Rated frequency	400 Hz
Rated speed	11 200 rpm
Stator and rotor resistance	0.015 pu
Stator and rotor reactance	0.1 pu
Unsaturated magnetizing reactance	3 pu
Normalized inertia	0.2 s

quency is controlled so that the slip, the difference between the converter frequency and the actual rotor speed, corresponds to the desired amount and direction of power flow to the machine. Fig. 5 shows the block diagram of this slip controller. Fig. 6 shows system waveforms as the slip frequency is controlled from zero to its rated value and then reduced steadily to the rated negative value. In the process, it can be noted that the machine electromagnetic torque goes through a range of zero to full positive and then is reversed to full negative at which point the machine is operating as a generator feeding power back to the high-frequency link. Note the near-sinusoidal waveform of the motor line current. This simulation result demonstrates the following.

1) There is no fundamental difficulty in having the proposed PDM converter operate an induction machine either as a motor or a generator.
2) Slip control strategy is adequate to change direction of power flow to the machine.
3) Synthesized voltages do not contain troublesome lower order harmonics. Higher order distortion has no significant effect on machine operation. Thus, no filters are needed between the PDM converter and the machine.

Adaptation to Single-Phase AC and DC

The power conversion technique of zero voltage switching with PDM control can be used to synthesize

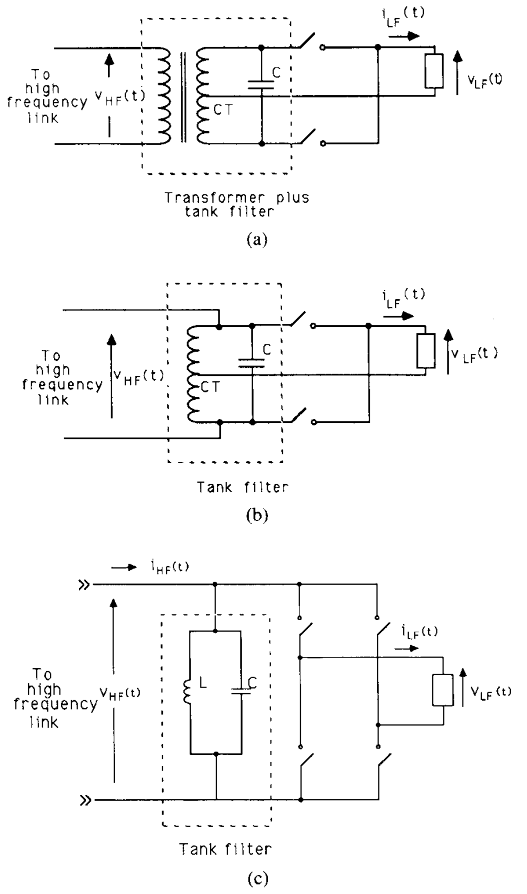


Fig. 7. Power circuits for single-phase PDM converter. (a) Center-tapped transformer half bridge. (b) Center-tapped inductor half bridge. (c) Full bridge.

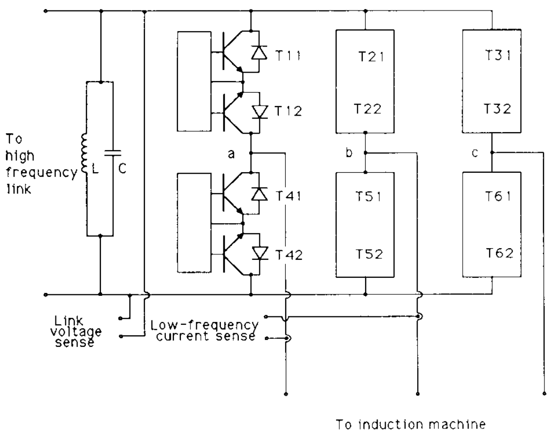


Fig. 8. Breadboard realization of three-phase PDM bridge. Component values given in Table III.

any low-frequency waveform that meets the frequency and amplitude limits discussed earlier. Suitable power circuits are derivatives of the three-phase ac bridge described above. Fig. 7 shows possible circuits suitable for synthesis of single-phase ac or dc with full four-quadrant V-I characteristics at the low-frequency end. It has previously been mentioned that the reference signal supplied to the PDM controller determines whether an ac or dc waveform is generated at the low-frequency end. Similarly, if a current source instead of a voltage source is desired at the low-frequency end, then the feedback signal to the PDM controller is changed to the resulting low-frequency current [9]. Additional impedance may be necessary in some cases to limit the ripple current on the low-frequency side.

VI. EXPERIMENTAL VERIFICATION

To demonstrate hardware feasibility and to provide experimental verification of the converter computer model a 5-kW laboratory breadboard of the proposed PDM converter has been built and operated successfully. In the breadboard system, a parallel-output series-resonant (POSR) converter [4], [10] operating from a rectified 60-Hz supply provides the high-frequency sinusoidal "link" voltage from which a three-phase PDM bridge converter operates to supply three-phase passive loads or an induction machine.

Fig. 8 shows the power circuit of the laboratory PDM bridge converter. Although it is sensitive to the reverse recovery characteristics of the internal diodes the two-transistor inverse-series realization was used for the bidirectional switches because it minimizes the number of power interconnections and because power Darlingtons are readily available. Table III gives important component values used in this breadboard.

A parallel *LC* tank circuit tuned to the link frequency is used as the link side filter. For the tank capacitor, General Electric 97F85 series polypropylene film capacitors have been used because of their high current ratings and a very low dissipation factor. For tank inductor, a litz wire wound inductor with a ferrite core was used. The overall Q of the tank circuit was measured to be about 160 for link voltage of 318 V rms and a link frequency of 19.32 kHz.

The feedback signals required by the AC–PDM control are obtained indirectly by sensing the link voltage with a signal transformer and applying to this isolated and scaled signal the same logic that controls the power circuit of the bridge. In this manner, the difficult task of feeding back the actual pole voltages has been avoided.

An open-loop constant volts/hertz type controller was built to allow operation of an induction machine from the breadboard converter. This controller supplies the PDM controller with the frequency and amplitude commands required for synthesizing the low-frequency voltages impressed on the machine. A soft start and a current limit were also added.

Fig. 9 shows typical voltage and current waveforms observed across one converter switch. The waveforms demonstrate the zero voltage switching of the PDM converters. Line voltage and current waveforms during soft start of a 60-Hz 220-V induction machine fed from a PDM bridge converter are shown in Fig. 10. The same set of

TABLE III
COMPONENT VALUES FOR THE BREADBOARD PDM CONVERTER OF FIG. 8

Component	Circuit Symbol	Key Specifications	Comments
Power Darlingtons	$T11$–$T62$	50 A, $V_{\mathrm{ceo(sus)}} = 500$, $V_{\mathrm{cev}} = 700$ V, $t_s = 5$ μs	MJE 10016
Snubber capacitor	$C1$–$C6$	0.047 μF, 1200 VDC	Sprague 715P series
Filter capacitor	C_T	3.0 μF, 1000 Vpk, 114 A	Three GE97F8522FC
Filter inductor	L_T	22.5 μH, 120 A	Litz wire, Ferrite core
Current sensors		100 A, 1000:1, DC-100 kHz	LEM LT 100-S

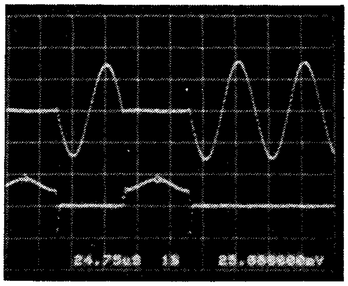


Fig. 9. Typical voltage and current waveforms observed across one switch of PDM converter (see Fig. 8). Upper trace: switch voltage, 250 V/div. Lower trace: switch current, 5 A/div.

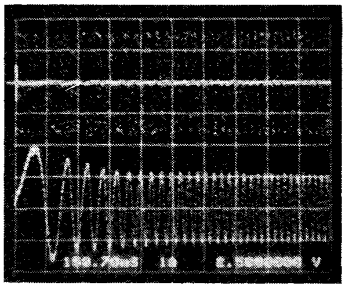


Fig. 10. Machine voltage and current waveforms during soft start with 230-V 60-Hz induction machine. Upper trace: line voltage v_{ab}, 250 V/div. Lower trace: line current i_a, 5 A/div.

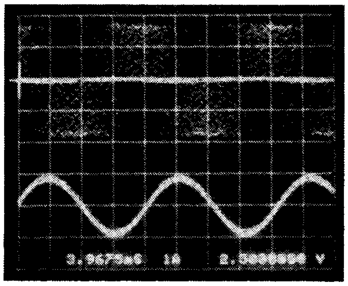


Fig. 11. Typical set of machine voltage and current waveforms observed on breadboard. Upper trace: line voltage v_{ab}, 250 V/div. Lower trace: line current i_a, 5 A/div.

waveforms is shown in Fig. 11 for no-load steady-state condition of operation of the machine. Fig. 12 shows the frequency spectrum of the waveforms of Fig. 11. Note that the lower order harmonics in either spectrum are very small. This is in agreement with similar results observed

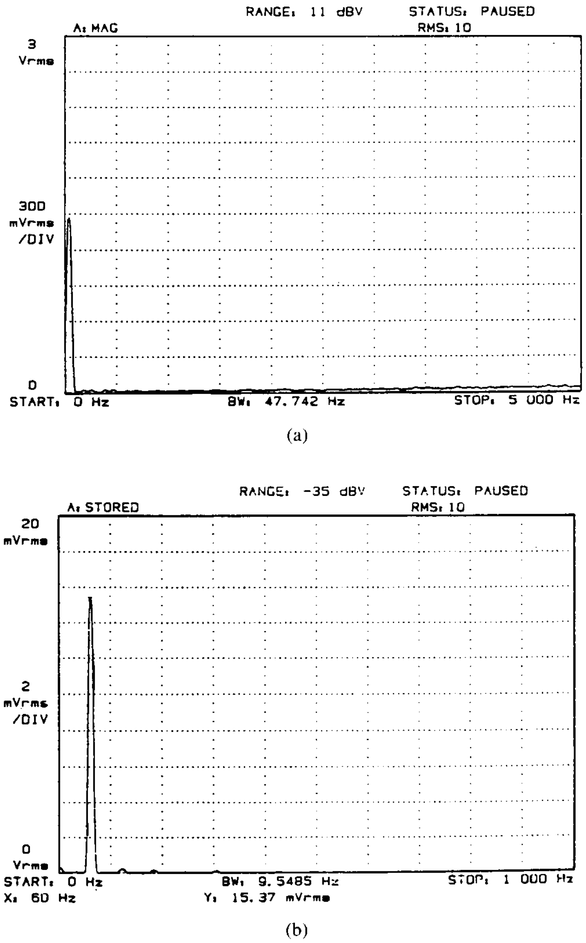


Fig. 12. Spectra of machine voltage and current. (a) Spectrum of line voltage v_{ab}, 300 V full scale. (b) Spectrum of line current i_a, 4 A full scale.

in simulated operation with the induction machine and with experimentally observed waveforms for other conditions of PDM synthesis, including three-phase passive loading [9]. The results of Fig. 12 demonstrate that an induction machine can be operated directly from a PDM converter with minimal influence of the harmonics on torque production and power flow in the machine. Also, the low-level audible noise expected from the motor as a result of the distributed spectral characteristics of the distortion over the audible range has been experimentally verified. The noise observed on the breadboard system had the characteristics of what can be described as low-level hiss. Such noise is much easier to tolerate than the loud tonal noise generally observed with PWM converter fed machines.

VII. CONCLUSIONS

The PDM converters have some very fashionable characteristics that make them an excellent candidate for the role of interface converters in a high-frequency (approximately 20 kHz) link power conversion system. The basic PDM converter is capable of high conversion efficiencies due to its one-stage power handling and low switching losses. It is capable of inherent bidirectional power flow requiring no changes in the power or the control circuit to effect a change in the direction of power flow. Operation directly off a 20-kHz link gives the PDM converter an equivalent switching rate of forty thousand switches per second. As a result, PDM converters have very high bandwidths, can synthesize signals with very few lower order harmonics, and can readily generate fundamental frequencies as high as 1000 Hz. Finally, a generalized power structure and an unrestrictive control scheme make the PDM converter very versatile so that it can interface a wide variety of loads and sources to the high-frequency link.

REFERENCES

[1] I. G. Hansen, "Description of a 20 kilohertz power distribution system," presented at 21st Intersociety Energy Conversion Engineering Conf. (IECEC), San Diego, Aug. 1986.

[2] A. C. Hoffman, I. G. Hansen, R. F. Beach, *et al.*, "Advanced secondary power system for transport aircraft," NASA Technical Paper 2463, 1985.

[3] P. K. Sood and T. A. Lipo, "Power conversion distribution system using a high-frequency ac link," *IEEE Trans. Ind. Appl.*, vol. 24, pp. 288-300, Mar/Apr. 1988.

[4] J. Mildice and L. Wappes, "Resonant ac power system proof-of-concept," NADA CR-175069, 1986.

[5] T. A. Lipo and P. K. Sood, "Study of the generator/motor operation of induction machines in a high-frequency link space power system," NASA report. Contract no. NAG3-631, Sept. 1986.

[6] T. Natarajan, "An evaluation of inverter topologies for high power spacecraft," presented at 21st Intersociety Energy Conversion Engineering Conf. (IECEC), San Diego, Aug. 1986.

[7] D. M. Divan, "The resonant dc link converter—A new concept in static power conversion," in *Conf. Rec. 1986 Annu. Meet. IEEE Ind. Appl. Soc.*, pp. 648-655.

[8] K. H. Liu and F. C. Lee, "Zero voltage switching technique in dc/dc converters," *IEEE Power Electronics Specialists Conf. Rec.*, pp. 58-70, 1986.

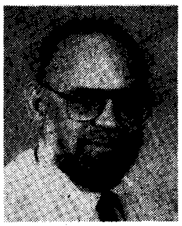
[9] P. K. Sood, "High-frequency link power conversion system," Ph.D. dissertation, University of Wisconsin—Madison, 1987.

[10] N. Mapham, "An SCR inverter with good regulation and sine-wave output," *IEEE Trans. Ind. Gen. Appl.*, vol. IGA-3, pp. 176-187, Mar./Apr. 1967.

Pradeep K. Sood (S'82-M'85-S'86-M'87) received the B.S. degree from the Indian Institute of Technology, Kanpur, India, the M.S. degree from Loughborough University of Technology, Loughborough, England, and the Ph.D. degree from the University of Wisconsin—Madison, in 1974, 1977, and 1987, respectively, all in electrical engineering.

In 1974 he joined the Research and Development division of the Indian Telephone Industries, Allahabad, India, working on the development of dc-to-dc converters for telephone systems. In 1977 he joined GEC Rectifiers, Stafford, England, where he was associated with the development of static converters. From 1978 to 1982 he was with the Universidade Federal da Paraiba, Campina Grande, Brazil, where he was engaged in teaching and research in the area of power conversion and motor drives. He is currently with the Electronic Speed Control Division of Emerson Electric Co., St. Louis, MO.

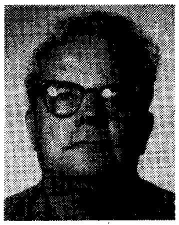
Dr. Sood is a member of Sigma Xi.



Thomas A. Lipo (M'64-SM'71-F'87) received the B.E.E. and M.S.E.E. degrees from Marquette University, Milwaukee, WI, in 1962 and 1964, respectively, and the Ph.D. degree in electrical engineering from the University of Wisconsin in 1968.

From 1969 to 1979 he was an Electrical Engineer in the Power Electronics Laboratory of Corporate R&D, General Electric Co. He is currently a Professor in the Department of Electrical and Computer Engineering, University of Wisconsin—Madison.

Dr. Lipo holds eight patents, has published over 100 papers and has received seven prize paper awards for his work. He is an active member of five IEEE Committees or Subcommittees and is past Chairman of two of them. He is a member of the Executive Board of the Industrial Applications Society and Editor of the IEEE TRANSACTIONS ON POWER ELECTRONICS.



Irving G. Hansen was born in Toledo, Ohio, in 1932. He received the B.S. degree in electrical engineering from Tri-State College, Angola, Indiana, in 1957, and the Masters of Engineering Science degree from the University of Toledo, Toledo, OH, in 1978.

He is currently a Senior Electrical Engineer at the NASA Lewis Research Center, Cleveland, OH, working in advanced technology for aerospace power systems. He holds two patents in aerospace instrumentation and has published fifteen articles on power electronics, components, and instrumentation.